A turbo SDMA receiver for strongly nonlinearly distorted MC-CDMA signals

Un récepteur turbo SDMA à signaux MC-CDMA soumis à de fortes distorsions non linéaires

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This paper considers the use of space division multiple access (SDMA) techniques for the uplink of multi-carrier code division multiple access (MC-CDMA) systems, where the transmitted signals face strong nonlinear distortion effects. The signal transmitted by each mobile terminal (MT) is submitted to a nonlinear operation consisting of a clipping device followed by a frequency-domain filtering operation, so as to reduce the envelope fluctuations and peak-to-mean envelope power ratio (PMEPR) while maintaining the spectral occupation of conventional MC-CDMA signals. At the base station, an iterative receiver employing multiple antennas jointly performs turbo multi-user detection and the estimation and cancellation of nonlinear distortion effects. Performance results show that the proposed receiver structure can achieve good performances that are very close to those obtained with linear transmitters, even for high system load and/or when a very low-PMEPR MC-CDMA transmission is intended for each MT.

Cet article envisage l’utilisation des techniques de division spatiale à accès multiple ou SDMA en voie montante pour les systèmes à accès multiple par répartition en codes multiporteuses ou MC-CDMA où le signal transmis est soumis à de fortes distorsions non linéaires. Le signal transmis par chaque terminal mobile est soumis à une opération non linéaire consistant d’un dispositif de coupure suivi d’une opération de filtrage au niveau du domaine de fréquence de manière à réduire les fluctuations de l’enveloppe ainsi que le rapport pic-moyenne de la puissance de l’enveloppe (PMEPR), tout en maintenant l’occupation spectrale des signaux MC-CDMA conventionnels. À la station de base, un récepteur itératif utilisant simultanément plusieurs antennes fait la détection multi-utilisateur ainsi que l’estimation et l’annulation des effets de distortion non linéaires. Les résultats montrent que les structures de récepteur proposées conduisent à de bonnes performances très proches de celles obtenues avec les transmetteurs linéaires, et cela même pour les systèmes à charge élevée et/ou quand une transmission MC-CDMA à très bas PMEPR est prévue pour chaque station de base.

Keywords: multi-carrier code division multiple access (MC-CDMA); multi-user detection; nonlinear effects; space division multiple access (SDMA); turbo equalization

I Introduction

Space division multiple access (SDMA) techniques employ multiple antennas to substantially increase the system capacity [2]. In this paper we consider the use of SDMA techniques for the uplink of multi-carrier code division multiple access (MC-CDMA) systems. As in other multi-carrier schemes, MC-CDMA signals have strong envelope fluctuations and high peak-to-mean envelope power ratio (PMEPR) values, leading to amplification difficulties. For this reason, it is desirable to reduce the envelope fluctuations of the transmitted signals. This is particularly important for the uplink transmission, since an efficient, low-cost power amplification is desirable at the mobile terminal (MT). Several techniques have been recommended to reduce the envelope fluctuations of multi-carrier signals (see [2] and references therein). One promising approach is to employ clipping techniques combined with frequency-domain filtering so as to reduce the envelope fluctuations of the transmitted signals while maintaining the spectral occupation of conventional schemes [2]. However, the nonlinear distortion effects can be severe when a low-PMEPR transmission is intended [2]–[3].

As in other CDMA schemes, since the transmission over time-dispersive channels destroys the orthogonality between users, a frequency-domain equalizer (FDE) is required before the despread-

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1 An MMSE FDE might also lead to noise correlations, creating unwanted dependencies between the decisions made for each data symbol associated with a given spreading code. This is usually not a problem in coded systems, provided that a suitable interleaving is employed between the channel encoder and the symbol mapper.
fine an iterative receiver that jointly performs turbo MUD as well as estimation and cancellation of nonlinear distortion effects, taking into account the frequency distribution of the distortion that is inherent to the transmitted signals.

This paper is organized as follows: The system characterization considered here is described in Section II. In Section III, we describe the iterative receivers proposed in this paper. Section IV presents a set of performance results, and Section V is concerned with the conclusions of the paper.

II System characterization

We consider the uplink transmission of MC-CDMA signals employing frequency-domain spreading. We have an SDMA architecture depicted in Fig. 1, corresponding to a multiple-input, multiple-output (MIMO) system with \( P \) users (MTs) transmitting independent data blocks and \( L \) receive antennas at the base station (BS). It is assumed that each MT has a single transmit antenna. The coded bits are interleaved and mapped, leading to the block of data symbols to be transmitted by the \( p \)-th MT \( \{ S_{k,p}; k = 0, 1, \ldots, N - 1 \} \), and a nonlinear self-interference one, i.e., \( S_{k,p} = \alpha_p S_{k,p} G_k + D_{k,p} G_k \), where \( \alpha_p \) is a scalar factor, defined in [7] and [8]; \( G_k, k = 0, 1, \ldots, N' - 1 \), are the frequency-domain filtering coefficients required to reduce the out-of-band radiation levels inherent to the nonlinear operation; and \( \{ D_{k,p}; k = 0, 1, \ldots, N' - 1 \} \) is the frequency-domain block of nonlinear self-interference components associated with the \( p \)-th MT. Unless otherwise stated, we will assume that \( G_k = 1 \) for the \( N \) in-band subcarriers and 0 for the \( N' - N \) out-of-band subcarriers, i.e., the spectral occupation of the transmitted signal is similar to the spectral occupation of conventional MC-CDMA signals. In this case, \( S_{k,p} = \alpha_p S_{k,p} + D_{k,p} \) for the \( N \) in-band subcarriers, and 0 otherwise. It can be shown that \( D_{k,p} \) is approximately Gaussian-distributed with zero mean; moreover, \( E[|D_{k,p}|^2] \) can be computed analytically, as described in [7] and [8].

III Receiver structure

III.A Linear transmitters

As usual, it is assumed that the length of the cyclic prefix (CP) is higher than the length of the overall channel impulse response. The received time-domain block associated with the \( l \)-th diversity branch, after the samples associated with the CP are discarded, is \( \{ y_{l,n}^0; n = 0, 1, \ldots, N - 1 \} \). The corresponding frequency-domain block (i.e., the length-\( N \) DFT of the block \( \{ y_{l,n}^0; n = 0, 1, \ldots, N - 1 \} \) is \( \{ Y_{k,l}^0; k = 0, 1, \ldots, N - 1 \} \).

Let us consider first a linear transmitter. In this case, the frequency-domain block transmitted by the \( p \)-th MT is \( \{ S_{k,p}^T = S_{k,p}; k = 0, 1, \ldots, N' - 1 \} \) and

\[
Y_{k,l}^0 = \sum_{n=1}^{P} S_{k,p}^T H_{k,p}^{Ch(l)} + N_{k}^0
\]

\[
= \sum_{n=1}^{P} A_{k,mod} M_{p} C_{k,p} \xi_{p} H_{k,p}^{Ch(l)} + N_{k}^0
\]

\[
= \sum_{n=1}^{P} A_{k,mod} M_{p} H_{k,p}^{Ch(l)} + N_{k}^0,
\]  

with \( H_{k,p}^{Ch(l)} \) denoting the channel frequency response between the \( p \)-th MT and the \( l \)-th diversity branch at the \( k \)-th subcarrier; \( N_{k}^0 \) denoting the corresponding noise channel response; and \( H_{k,p}^{Ch(l)} \) representing \( C_{k,p} \). To detect the \( k \)-th symbol of the \( p \)-th MT, we will use the set of subcarriers \( \Psi_k \), for the \( l \)-th antenna, and \( A(k) = [A_{k,mod} M_{1,1} \ldots A_{k,mod} M_{p,1}]^T \), we have

\[
Y(k) = \mathbf{H}^T(k) A(k) + \mathbf{N}(k),
\]  

where \( (\cdot)^T \) denotes the transpose matrix and \( \mathbf{N}(k) = [\mathbf{N}^0(k) \cdots \mathbf{N}^L(k)]^T \), with \( \mathbf{N}^0(k) \) denoting the column vector with the noise samples associated with the set of frequencies \( \Psi_k \), for the \( l \)-th antenna. In (2), \( \mathbf{H}(k) \) is the overall channel matrix associated with \( A(k) \), i.e., \( \mathbf{H}(k) = [A^1(k) \cdots A^L(k)] \), with

![Figure 1: System characterization.](image-url)